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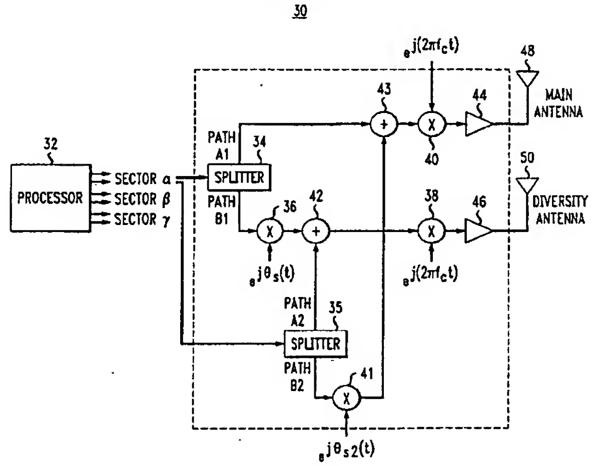
(54) Symmetric sweep phase sweep transmit diversity

(57) Described herein is a method and apparatus for transmission that provides the performance of space time spreading (STS) or orthogonal transmit diversity (OTD) and the backwards compatibility of phase sweep transmit diversity (PSTD) without degrading performance of either STS or PSTD using a symmetric sweep PSTD transmission architecture. In one embodiment, a pair of signals s_1 and s_2 are split into signals $s_1(a)$ and $s_1(b)$ and signals $s_2(a)$ and $s_2(b)$, respectively. Signal s_1 comprises a first STS/OTD signal belonging to an STS/OTD pair, and signal s_2 comprises a second STS/OTD signal belonging to the STS/OTD pair. Signals $s_1(b)$ and $s_2(b)$ are phase swept using a pair of phase sweep frequency signals that would cancel out any self induced interference. For example, the pair of phase sweep frequency signals utilize a same phase sweep frequency with one of the phase sweep frequency signals rotating in the opposite direction plus an offset of π relative to the other phase sweep frequency signal. The resultant phase swept signals $s_1(b)$ and $s_2(b)$ are added to signals $s_2(a)$ and $s_1(a)$ before being amplified and transmitted.

FIG. 3



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Description

Background of the Related Art

[0001] Performance of wireless communication systems is directly related to signal strength statistics of received signals. Third generation wireless communication systems utilize transmit diversity techniques for downlink transmissions (i.e., communication link from a base station to a mobile-station) in order to improve received signal strength statistics and, thus, performance. Two such transmit diversity techniques are space time spreading (STS) and phase sweep transmit diversity (PSTD).

[0002] FIG. 1 depicts a wireless communication system 10 employing STS. Wireless communication system 10 comprises at least one base station 12 having two antenna elements 14-1 and 14-2, wherein antenna elements 14-1 and 14-2 are spaced far apart for achieving transmit diversity. Base station 12 receives a signal S for transmitting to mobile-station 16. Signal S is alternately divided into signals s_e and s_o, wherein signal s_e comprises even data bits and signal s_o comprises odd data bits. Signals s_e and s_o are processed to produce signals S^{14-1} and S^{14-2}. Specifically, s_e is multiplied with Walsh code w_1 to produce signal $s_e w_1$; a conjugate of signal s_o is multiplied with Walsh code w_2 to produce signal $s_o{}^*w_2$; signal s_o is multiplied with Walsh code w_1 to produce $s_o w_1$; and a conjugate of signal s_e is multiplied with Walsh code w_2 to produce $s_e{}^*w_2$. Signal $s_e w_1$ is added to signal $s_o{}^*w_2$ to produce signal S^{14-1} (i.e., $S^{14-1}=s_e w_1+s_o{}^*w_2$) and signal $s_e{}^*w_2$ is subtracted from signal $s_o w_1$ to produce signal S^{14-2} (i.e., $S^{14-2}=s_o w_1-s_e{}^*w_2$). Signals S^{14-1} and S^{14-2} are transmitted at substantially equal or identical power levels over antenna elements 14-1 and 14-2, respectively. For purposes of this application, power levels are "substantially equal" or "identical" when the power levels are within 1% of each other.

[0003] Mobile-station 16 receives signal R comprising $\gamma_1(S^{14-2})+\gamma_2(S^{14-2})$, wherein γ_1 and γ_2 are distortion factor coefficients associated with the transmission of signals S^{14-1} and S^{14-2} from antenna elements 14-1 and 14-2 to mobile-station 16, respectively. Distortion factor coefficients γ_1 and γ_2 can be estimated using pilot signals, as is well-known in the art. Mobile-station 16 decodes signal R with Walsh codes w_1 and w_2 to respectively produce outputs:

$$W_1=\gamma_1 s_e+\gamma_2 s_o \quad \text{equation 1}$$

$$W_2=\gamma_1 s_o{}^*-\gamma_2 s_e{}^* \quad \text{equation 1a}$$

Using the following equations, estimates of signals s_e and s_o, i.e., $\hat{S}_e$ and $\hat{S}_o$, may be obtained:

$$\hat{s}_e = \gamma_1^*W_1 - \gamma_2 W_2^* = s_e\left(|\gamma_1|^2 + |\gamma_2|^2\right) + noise \quad \text{equation 2}$$

$$\hat{s}_o = \gamma_2^*W_1 + \gamma_1 W_2^* = s_o\left(|\gamma_1|^2 + |\gamma_2|^2\right) + noise' \quad \text{equation 2a}$$

[0004] However, STS is a transmit diversity technique that is not backward compatible from the perspective of the mobile-station. That is, mobile-station 16 is required to have the necessary hardware and/or software to decode signal R. Mobile-stations without such hardware and/or software, such as pre-third generation mobile-stations, would be incapable of decoding signal R.

[0005] By contrast, phase sweep transmit diversity (PSTD) is backward compatible from the perspective of the mobile-station. FIG. 2 depicts a wireless communication system 20 employing PSTD. Wireless communication system 20 comprises at least one base station 22 having two antenna elements 24-1 and 24-2, wherein antenna elements 24-1 and 24-2 are spaced far apart for achieving transmit diversity. Base station 22 receives a signal S for transmitting to mobile-station 26. Signal S is evenly power split into signals s_1 and s_2 and processed to produce signals S^{24-1} and S^{24-2}, where $s_1=s_2$. Specifically, signal s_1 is multiplied by Walsh code w_k to produce $S^{24-1}=s_1 w_k$, where k represents a particular user or mobile-station. Signal s_2 is multiplied by Walsh code w_k and a phase sweep frequency signal $e^{j2\pi fst}$ to produce S^{24-2}, i.e., $S^{24-2}=s_2 w_k e^{j2\pi f_s t}=s_1 w_k e^{j2\pi f_s t}=S^{24-1}\, e^{j2\pi f_s t}$, where f_s is a phase sweep frequency and t is time.

[0006] Signals S^{24-1} and S^{24-2} are transmitted at substantially equal power levels over antenna elements 24-1 and 24-2, respectively. Note that the phase sweep signal $e^{j2\pi fst}$ is being represented in complex baseband notation, i.e., $e^{j2\pi f_s t}= \cos(2\pi f_s t)+j\sin(2\pi f_s t)$. It should be understood that the phase sweep signal may also be applied at an interme-

diate frequency or a radio frequency.

[0007] Mobile-station 26 receives signal R comprising $\gamma_1 S^{24-1}+\gamma_2 S^{24-2}$. Simplifying the equation for R results in

$$R = \gamma_1 S^{24-1} + \gamma_2 S^{24-1} e^{j2\pi f_s t} \qquad \text{equation 3}$$

$$R = S^{24-1} \{\gamma_1 + \gamma_2 e^{j2\pi f s t}\} \qquad \text{equation 3a}$$

$$R = S^{24-1} \gamma_{eq} \qquad \text{equation 3b}$$

where γ_{eq} is an equivalent channel seen by mobile-station 26. Distortion factor coefficient γ_{eq} can be estimated using pilot signals and used, along with equation 3b, to obtain estimates of signal s_1 and/or s_2.

[0008] In slow fading channel conditions, both transmit diversity techniques, i.e., STS and PSTD, improve performance (relative to when no transmit diversity technique is used) by making the received signal strength statistics associated wit a slow fading channel at the receiver look like those associated with a fast fading channel. However, PSTD does not provide the same amount of overall performance improvement as STS. Accordingly, there exists a need for a transmission technique that provides the performance of STS and the backwards compatibility of PSTD without degrading performance of either STS or PSTD.

Summary of the Invention

[0009] The present invention is a method and apparatus for transmission that provides the performance of space time spreading (STS) or orthogonal transmit diversity (OTD) and the backwards compatibility of phase sweep transmit diversity (PSTD) without degrading performance of either STS or PSTD using a symmetric sweep PSTD transmission architecture, which involves phase sweeping a pair of signals having a pair of STS/OTD signals. In one embodiment, a pair of signals s_1 and s_2 are split into signals s_1(a) and s_1(b) and signals s_2(a) and s_2(b), respectively. Signal s_1 comprises a first STS/OTD signal belonging to an STS/OTD pair, and signal s_2 comprises a second STS/OTD signal belonging to the STS/OTD pair. Signals s_1(b) and s_2(b) are phase swept using a pair of phase sweep frequency signals that would cancel out any self induced interference caused by phase sweeping both signals s_1(b) and s_2(b). For example, the pair of phase sweep frequency signals utilize a same phase sweep frequency with one of the phase sweep frequency signals rotating in the opposite direction plus an offset of π relative to the other phase sweep frequency signal. The resultant phase swept signals s_1(b) and s_2(b) are added to signals s_2(a) and s_1(a) before being amplified and transmitted.

Brief Description of the Drawings

[0010] The features, aspects, and advantages of the present invention will become better understood with regard to the following description, appended claims, and accompanying drawings where

FIG. I depicts a wireless communication system employing space time spreading techniques in accordance with the prior art;

FIG. 2 depicts a wireless communication system employing phase sweep transmit diversity in accordance with the prior art; and

FIG. 3 depicts a base station employing symmetric sweep phase sweep transmit diversity in accordance with one embodiment of the present invention;

FIG. 4 depicts a base station employing symmetric sweep phase sweep transmit diversity in accordance with another embodiment of the present invention; and

FIG. 5 depicts a base station employing symmetric sweep phase sweep transmit diversity in accordance with another embodiment of the present invention.

Detailed Description

[0011] FIG. 3 depicts a base station 30 employing symmetric sweep phase sweep transmit diversity in accordance with the present invention, wherein symmetric sweep phase sweep transmit diversity utilizes code division multiple access (CDMA), phase sweep transmit diversity (PSTD), and space time spreading (STS) or orthogonal transmit di-

versity (OTD) techniques. CDMA, PSTD, STS and OTD are well-known in the art.

[0012] Base station 30 provides wireless communication services to mobile-stations, not shown, in its associated geographical coverage area or cell, wherein the cell is divided into three sectors α, β, γ. Note that the base station could be divided into an arbitrary number of sectors and not change the invention described here. Base station 30 includes a transmission architecture that incorporates STS or OTD and biased PSTD, as will be described herein.

[0013] Base station 30 comprises a processor 32, splitters 34, 35, multipliers 36, 38, 40, 41, adders 42, 43, amplifiers 44, 46, and a pair of diversity antennas 48, 50. Note that base station 30 also includes configurations of splitters, multipliers, adders, amplifiers and antennas for sectors β, γ that are identical to those for sector α. For simplicity sake, the configuration for sectors β, γ are not shown. Additionally, for discussion purposes, it is assumed that signals S_k are intended for mobile-stations k located in sector α and, thus, the present invention will be described with reference to signals S_k being processed for transmission over sector α.

[0014] Processor 32 includes software for processing signals S_k in accordance with well-known CDMA and STS/OTD techniques. The manner in which a particular signal S_k is processed by processor 32 depends on whether mobile-station k is STS/OTD compatible, i.e., mobile-station capable of decoding signals processed using STS/OTD. Processor 32 may also include software for determining whether mobile-station k is STS/OTD compatible. If mobile-station k is not STS/OTD compatible, then signal S_k is processed in accordance with CDMA techniques to produce signal S_{k-1}, which is also referred to herein as a non-STS/OTD signal S_{k-1}. Note that, in another embodiment, processor 32 is operable to process signals S_k in accordance with a multiple access technique other than CDMA, such as time or frequency division multiple access. In this embodiment, when mobile-station k is not STS/OTD compatible, then signal S_k is processed in accordance with such other multiple access technique to produce the non-STS/OTD signal S_{k-t}.

[0015] If mobile-station k is STS/OTD compatible, then signal S_k is processed in accordance with CDMA and STS/OTD. Specifically, if mobile-station k is STS compatible, then signal S_k is processed using STS. Such process includes alternately dividing signal S_k into signals s_e and s_o, wherein signal s_e comprises even data bits and signal s_o comprises odd data bits. Signal s_e is multiplied with Walsh code w_1 to produce signal $s_e w_1$, and a conjugate of signal s_e is multiplied with Walsh code w_2 to produce $s_e^* w_2$. Signal s_o is multiplied with Walsh code w_1 to produce $s_o w_1$, and a conjugate of signal s_o is multiplied with Walsh code w_2 to produce signal $s_o^* w_2$. Signal $s_e w_1$ is added to signal $s_o^* w_2$ to produce signal $S_{k-2}(a) = s_e w_1 + s_o^* w_2$. Signal $s_e^* w_2$ is subtracted from signal $s_o w_1$ to produce signal $S_{k-2}(b) = s_o w_1 - s_e^* w_2$. Signals $S_{k-2}(a)$, $S_{k-2}(b)$ are also referred to herein as STS signals, and together signals $S_{k-2}(a)$, $S_{k-2}(b)$ collectively comprise an STS pair.

[0016] If mobile-station k is OTD compatible, then signal S_k is processed using OTD. Orthogonal transmit diversity involves dividing signal S_k into signals s_e and s_o, and multiplying signals s_e and s_o using Walsh codes w_1, w_2 to produce signals $S_{k-3}(a)$, $S_{k-3}(b)$, i.e., $S_{k-3}(a)=s_e w_1$ and $S_{k-3}(b) = s_o w_2$, respectively. Signals $S_{k-3}(a)$, $S_{k-3}(b)$ are also referred to herein as OTD signals, and together signals $S_{k-3}(a)$, $S_{k-3}(b)$ collectively comprise an OTD pair.

[0017] For illustration purposes, the present invention will be described herein with reference to STS and signals $S_{k-2}(a)$, $S_{k-2}(b)$. It should be understood that the present invention is also applicable to OTD and signals $S_{k-3}(a)$, $S_{k-3}(b)$.

[0018] The output of processor 32 are signals $s_{\alpha-1}$, $s_{\alpha-2}$, where signal $s_{\alpha-1}$ comprises of signals S_{k-1} and $S_{k-2}(a)$ and signal $s_{\alpha-2}$ comprises of signals $S_{k-2}(b)$, i.e.,

$$s_{\alpha-1} = \sum S_{k-1} + \sum S_{k-2}(a) \text{ and } s_{\alpha-2} = \sum S_{k-2}(b).$$

[0019] That is, signals intended for STS compatible mobile-stations are included in both output signals $s_{\alpha-1}$, $s_{\alpha-2}$ and signals intended for non-STS compatible mobile-stations are included in only signal $s_{\alpha-1}$. Alternately, signal $s_{\alpha-1}$ comprises of signals S_{k-1} and $S_{k-2}(b)$ and signal $s_{\alpha-2}$ comprises of signals $S_{k-2}(a)$.

[0020] Signal $s_{\alpha-1}$ is split by splitter 34 into signals $s_{\alpha-1}(a)$, $s_{\alpha-1}(b)$ and processed along paths A1 and B1, respectively, by multipliers 36, 38, 40, adders 42, 43 and amplifiers 44, 46 in accordance with PSTD techniques. Signal $s_{\alpha-2}$ is split by splitter 35 into signals $s_{\alpha-2}(a)$, $s_{\alpha-2}(b)$ and processed along pathsA2 and B2, respectively, by multipliers 38, 40, 41, adders 42, 43 and amplifiers 44, 46 in accordance with PSTD techniques. Note that signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ are identical to respective signal $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$ in terms of data, and that signals $s_{\alpha-1}$, $s_{\alpha-2}$ may be evenly or unevenly split in terms of power.

[0021] Signals $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$ are provided as inputs into multipliers 36, 41 where signals $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$ are frequency phase swept with phase sweep frequency signals (JIMMY: I can't edit the equations, but change all of the "-" signs in the exponents to "+" signs in ALL e^j terms. Please change this in all of the figures as well. $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$ to produce signals $S_{36}=s_{\alpha-1}(b)e^{j\Theta_s(t)}$, $S_{41}=s_{\alpha-2}(b)e^{j\Theta_{s2}(t)}$, respectively, wherein $\Theta_s = 2\pi f_s t$, $e^{j\Theta_s(t)} = \cos(2\pi f_s t)+j\sin(2\pi f_s t)$, $\Theta_{s2} = -2\pi f_s t+\pi$, $e^{j\Theta_{s2}(t)}=-\cos(2\pi f_s t)+j\sin(2\pi f_s t)$, f_s represents a fixed or varying phase sweep frequency and t represents time.

[0022] Note that phase sweep frequency signals $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$ utilize a same phase sweep frequency with one of the

signals, i.e., $e^{j\Theta_{s2}(t)}$, rotating in the opposite direction plus an offset of π relative to the other signal, i.e., $e^{j\Theta_s(t)}$. If the phase sweep frequency signals $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$ were identical, i.e., $\Theta_s = \Theta_{s2}$, self induced interference would be generated by base station 30 that would degrade STS/OTD performance. By configuring the phase sweep signals $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$ to have this relationship, the self induced interference is canceled and STS/OTD performance is optimized.

[0023] Signal S_{41} is added to signal $s_{\alpha-1}(a)$ by adder 43 to produce signal $S_{43}= S_{41} + s_{\alpha-1}(a)= s_{\alpha-2}(b)e^{j\Theta_{s2}(t)} + s_{\alpha-1}(a)$. Signal S_{43} and carrier signal $e^{j2\pi f_c t}$ are provided as inputs into multiplier 40 to produce signal S_{40}, where $S_{40}=(s_{\alpha-2}(b)e^{j\Theta_{s2}(t)} + s_{\alpha-1}(a))e^{j2\pi f_c t}$, $e^{j2\pi f_c t} = \cos(2\pi f_c t)+j\sin(2\pi f_c t)$, and f_c represents a carrier frequency.

[0024] Signal S_{36} is added to signal $s_{\alpha-2}(a)$ by adder 42 to produce signal $S_{42}=s_{\alpha-1}(b)e^{j\Theta_s(t)} + s_{\alpha-2}(a)$. Signal S_{42} and carrier signal $e^{j2\pi f_c t}$ are provided as inputs into multiplier 38 to produce signal S_{38}, where $S_{38}=(s_{\alpha-1}(b)e^{j\Theta_s(t)} + s_{\alpha-2}(a))e^{j2\pi f_c t}$.

[0025] Signals S_{40}, S_{38} are amplified by amplifiers 44, 46 to produce signals S_{44} and S_{46} for transmission over antennas 48, 50, where signal $S_{44}=A_{44}((s_{\alpha-2}(b)e^{j\Theta_{s2}(t)}+ s_{\alpha-1}(a))\, e^{j2\pi f_c t})$, $S_{46}=A_{46}\,(s_{\alpha-1}(b)e^{j\Theta_s(t)} + s_{\alpha-2}(a))e^{j2\pi f_c t}$, A_{44} represents the amount of gain associated with amplifier 44 and A_{46} represents the amount of gain associated with amplifier 46.

[0026] In one embodiment, the amounts of gain A_{44}, A_{46} are substantially equal. In this embodiment, signals $s_{\alpha-1}$, $s_{\alpha-2}$ are split by splitters 34, 35 such that the power levels of signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ are substantially equal to the power levels of signal $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$. Advantageously, equal gain amplifiers can be used, which lowers the cost of base station 30 compared to base station cost when unequal amplifiers are used.

[0027] In another embodiment, the amounts of gain A_{44}, A_{46} are different and related to how splitters 34, 35 split signals $s_{\alpha-1}$, $s_{\alpha-2}$. Specifically, the amounts of gain A_{44}, A_{46} applied to signals S_{40}, S_{38} should be amounts that would cause the power levels of signals S_{44} and S_{46} to be approximately or substantially equal. For purposes of this application, power levels are "approximately equal" when the power levels are within 10% of each other.

[0028] FIG. 5 depicts a base station 70 employing symmetric sweep phase sweep transmit diversity in accordance with one embodiment of the present invention. In this embodiment, a form of PSTD referred to herein as split shift PSTD in also utilized. Split shift PSTD involves shifting both signals split from a single signal using phase sweep frequency signals that sweeps both signals in opposite direction. As shown in FIG. 5, signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ are phase swept by multipliers 37, 39 using phase sweep frequency signals $e^{-j\Theta_s(t)}$, $e^{-j\Theta_{s2}(t)}$, respectively. Although this embodiment depicts phase sweep frequency signals $e^{-j\Theta_s(t)}$, $e^{-j\Theta_{s2}(t)}$ equal and opposite to phase sweep frequency signals $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$, it should be understood that the phase sweep frequency signals used to phase sweep signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ need not be equal in magnitude. In another embodiment, signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ are phase swept using phase sweep frequency signals that result in phase swept signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$ with a desired or other phase difference to phase swept signals $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$. Note that that the phase sweep frequency signal used to phase sweep signals $s_{\alpha-1}(a)$, $s_{\alpha-2}(a)$, $s_{\alpha-1}(b)$, $s_{\alpha-2}(b)$ may be phase shifting at an identical or different rate from each other, may be phase shifting at fixed and/or varying rates, or may be phase shifting in the same or opposite direction.

[0029] Although the present invention has been described in considerable detail with reference to certain embodiments, other versions are possible. For example, phase sweeping could be performed on paths A1 and/or A2 instead of paths B1 and/or B2. In another example, the phase sweep frequency signals are interchanged. FIG. 4 depicts another embodiment of the present invention in which phase sweeping is performed along paths A1 and A2 instead of paths B1 and B2 and phase sweep frequency signals $e^{j\Theta_s(t)}$, $e^{j\Theta_{s2}(t)}$ are provided as inputs into multipliers 41, 36, respectively. Therefore, the scope of the present invention should not be limited to the description of the embodiments contained herein.

Claims

1. A method of signal transmission comprising the steps of:

splitting a signal s_1 into signals $s_1(a)$ and $s_1(b)$, wherein signal s_1 comprises a first STS/OTD signal belonging to an STS/OTD pair;

splitting a signal s_2 into signals $s_2(a)$ and $s_2(b)$, wherein signal s_2 comprises a second STS/OTD signal belonging to the STS/OTD pair;

phase sweeping the signal $s_1(b)$ using a first phase sweep frequency signal to produce a phase swept signal $s_1(b)$;

phase sweeping the signal $s_2(b)$ using a second phase sweep frequency signal to produce a phase swept signal $s_2(b)$, the first and second phase sweep frequency signals being configured to cancel out any self induced interference caused by phase sweeping the signals $s_1(b)$ and $s_2(b)$;

adding the phase swept signal $s_2(b)$ to the signal $s_1(a)$ to produce a summed signal s_3; and

adding the phase swept signal $s_1(b)$ to the signal $s_2(a)$ to produce a summed signal S_4.

2. The method of claim 1, wherein the first and second phase sweep frequency signals utilize a same phase sweep frequency with the second phase sweep frequency signal rotating in the opposite direction plus an offset of π relative to the first phase sweep frequency signal.

3. The method of claim 1, wherein the first and second phase sweep frequency signals utilize a same phase sweep frequency with the first phase sweep frequency signal rotating in the opposite direction plus an offset of π relative to the second phase sweep frequency signal.

4. The method of claim 1 comprising the additional steps of:

transmitting the summed signal s_3 over a first antenna belonging to a pair of diversity antennas; and
transmitting the summed signal s_4 over a second antenna belonging to the pair of diversity antennas.

5. The method of claim 1 comprising the additional steps of:

prior to the step of adding the phase swept signal $s_2(b)$ to the signal $s_1(a)$, phase sweeping the signal $s_1(a)$ using a third phase sweep frequency signal to produce a phase swept signal $s_1(a)$ with a different phase from the phase swept signal $s_2(b)$; and
prior to the step of adding the phase swept signal $s_1(b)$ to the signal $s_2(a)$, phase sweeping the signal $s_2(a)$ using a fourth phase sweep frequency signal to produce a phase swept signal $s_2(a)$ with a different phase from the phase swept signal $s_1(b)$.

6. A method of signal transmission comprising the steps of:

splitting a signal s_1 into signals $s_1(a)$ and $s_1(b)$, wherein signal s_1 comprises a first STS/OTD signal belonging to an STS/OTD pair;
splitting a signal s_2 into signals $s_2(a)$ and $s_2(b)$, wherein signal s_2 comprises a second STS/OTD signal belonging to the STS/OTD pair;
phase sweeping the signal $s_1(a)$ using a first phase sweep frequency signal to produce a phase swept signal $s_1(a)$;
phase sweeping the signal $s_2(a)$ using a second phase sweep frequency signal to produce a phase swept signal $s_2(a)$, the first and second phase sweep frequency signals being configured to cancel out any self induced interference caused by phase sweeping the signals $s_1(a)$ and $s_2(a)$;
adding the phase swept signal $s_2(a)$ to the signal $s_1(b)$ to produce a summed signal s_3; and
adding the phase swept signal $s_1(a)$ to the signal $s_2(b)$ to produce a summed signal s_4.

7. The method of claim 6, wherein the first and second phase sweep frequency signals utilize a same phase sweep frequency with the second phase sweep frequency signal rotating in the opposite direction plus an offset of π relative to the first phase sweep frequency signal.

8. The method of claim 6, wherein the first and second phase sweep frequency signals utilize a same phase sweep frequency with the first phase sweep frequency signal rotating in the opposite direction plus an offset of π relative to the second phase sweep frequency signal.

9. The method of claim 6 comprising the additional steps of:

transmitting the summed signal s_3 over a first antenna belonging to a pair of diversity antennas; and
transmitting the summed signal s_4 over a second antenna belonging to the pair of diversity antennas.

10. The method of claim 6 comprising the additional steps of:

prior to the step of adding the phase swept signal $s_2(a)$ to the signal $s_1(b)$, phase sweeping the signal $s_1(b)$ using a third phase sweep frequency signal to produce a phase swept signal $s_1(b)$ with a different phase from the phase swept signal $s_2(a)$; and
prior to the step of adding the phase swept signal si(a) to the signal $s_2(b)$, phase sweeping the signal $s_2(b)$ using a fourth phase sweep frequency signal to produce a phase swept signal $s_2(b)$ with a different phase from the phase swept signal $s_1(a)$.

FIG. 1

PRIOR ART

10

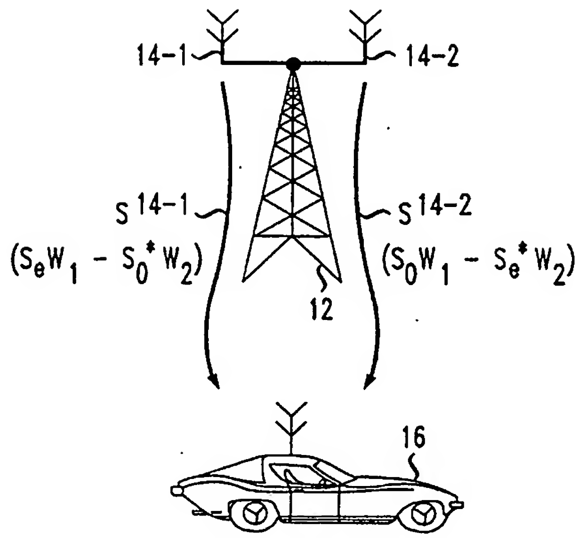


FIG. 2

PRIOR ART

20

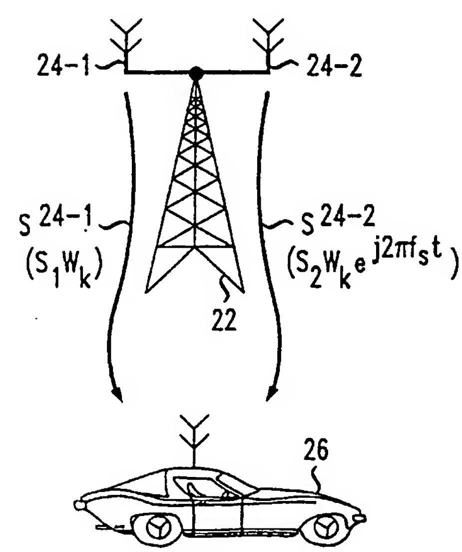


FIG. 3

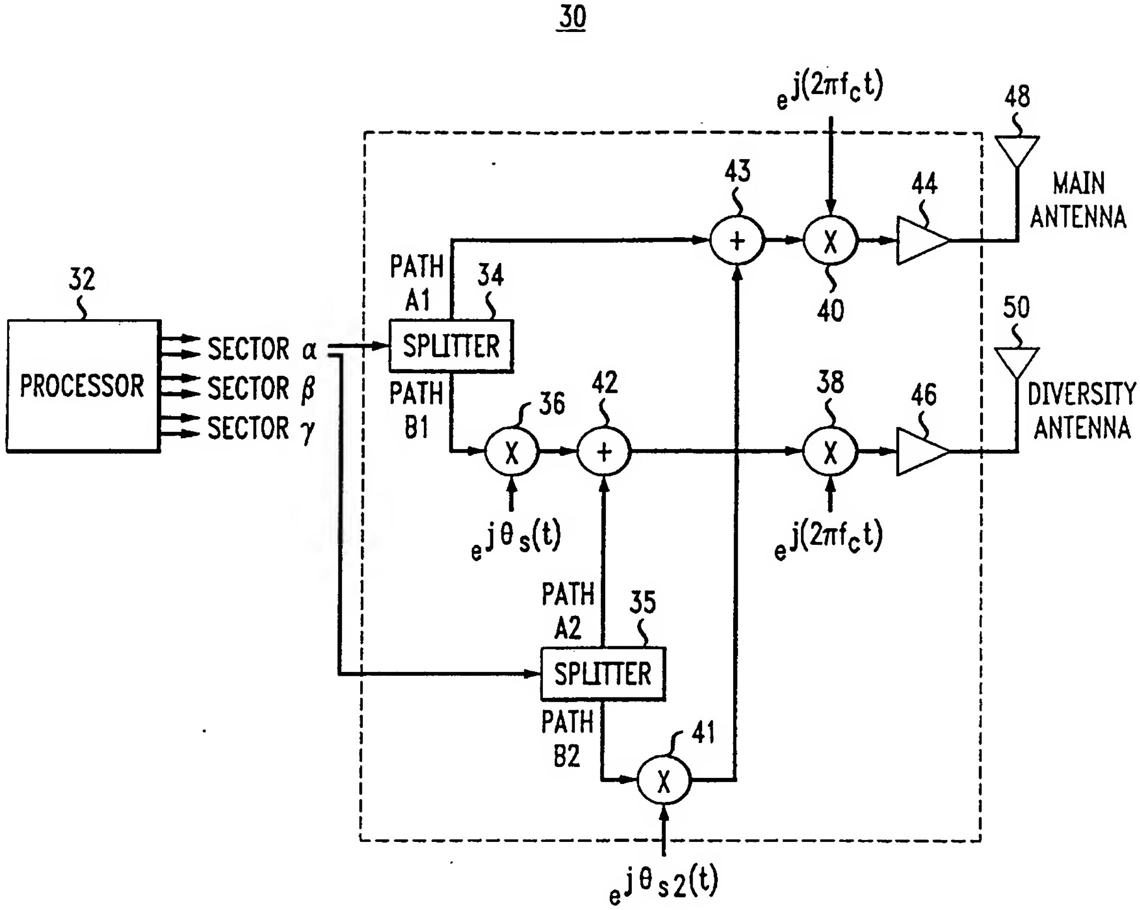

30
PROCESSOR
32
SECTOR α
SECTOR β
SECTOR γ
PATH A1
34
SPLITTER
PATH B1
36
42
38
46
43
40
44
48
MAIN ANTENNA
50
DIVERSITY ANTENNA
$e^{j(2\pi f_c t)}$
$e^{j(2\pi f_c t)}$
$e^{j\theta_s(t)}$
PATH A2
35
SPLITTER
PATH B2
41
$e^{j\theta_{s2}(t)}$

FIG. 4

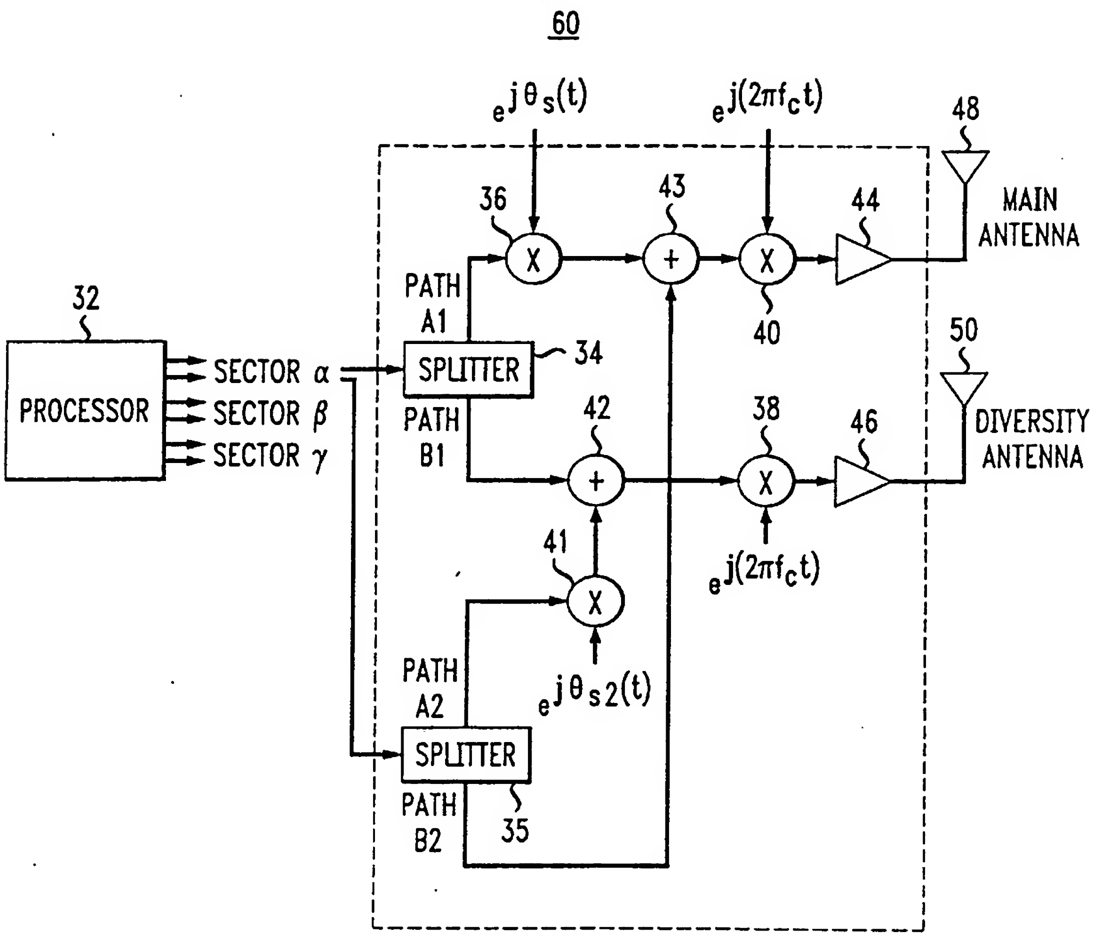
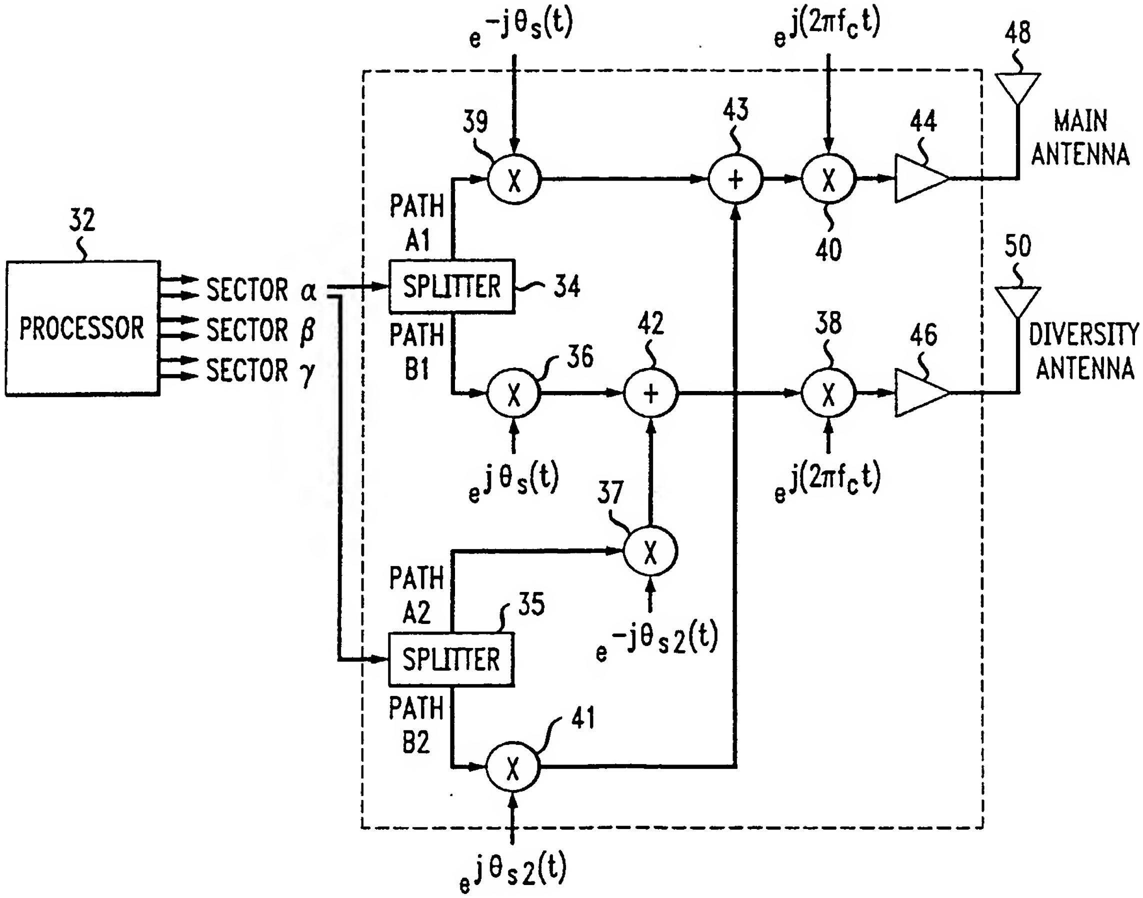

60
$e^{j\theta_s(t)}$
$e^{j(2\pi f_c t)}$
48
36
43
44
MAIN
ANTENNA
PATH
A1
40
32
50
34
SPLITTER
SECTOR α
PROCESSOR
SECTOR β
SECTOR γ
PATH
B1
42
38
46
DIVERSITY
ANTENNA
$e^{j(2\pi f_c t)}$
41
PATH
A2
$e^{j\theta_{s2}(t)}$
SPLITTER
PATH
B2
35

FIG. 5

70


PROCESSOR
32
SECTOR α
SECTOR β
SECTOR γ
SPLITTER
34
PATH A1
PATH B1
SPLITTER
35
PATH A2
PATH B2
$e^{-j\theta_s(t)}$
$e^{j(2\pi f_c t)}$
$e^{j\theta_s(t)}$
$e^{-j\theta_{s2}(t)}$
$e^{j\theta_{s2}(t)}$
36
37
38
39
40
41
42
43
44
46
48
MAIN ANTENNA
50
DIVERSITY ANTENNA

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EUROPEAN SEARCH REPORT

Application Number
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Place of search	Date of completion of the search	Examiner
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